

To illustrate how a  $Z-\theta$  transmission line chart can be used to determine the transmission characteristics of a sandwich, an example will be considered. For this example, the polarization is perpendicular to the plane of incidence,  $\lambda_0 = 3.2 \text{ cm} = 1.26 \text{ inch}$ ,  $\theta_0 = 45^\circ$ ,  $d_1 = 0.05 \text{ inch}$ ,  $\mu_1 = 1$ ,  $\epsilon_1 = 6$ ,  $d_2 = 0.21 \text{ inch}$ ,  $\mu_2 = 0.8(1 + j0.05)$ ,  $\epsilon_2 = 4(1 - j0.2)$ ,  $d_3 = 0.07 \text{ inch}$ ,  $\mu_3 = 1$ , and  $\epsilon_3 = 4$ . Now  $\eta_{0\perp} = \eta_{4\perp} = 1.414$ ,  $\eta_{1\perp} = 0.426$ ,  $\eta_{2\perp} = 0.481/7.9^\circ$ ,  $\eta_{3\perp} = 0.535$ ,  $\alpha_1 = \alpha_3 = 0$ ,  $\alpha_2 = 0.721 \text{ nepers per inch}$ ,  $\beta_1 = (2\pi)(1.861) \text{ radians per inch}$ ,  $\beta_2 = (2\pi)(1.317) \text{ radians per inch}$ , and  $\beta_3 = (2\pi)(1.485) \text{ radians per inch}$ .

The point  $Z_1 = \eta_{0\perp}/\eta_{1\perp} = 3.317$  is plotted on a  $Z-\theta$  chart, as in Fig. 2 (below). The

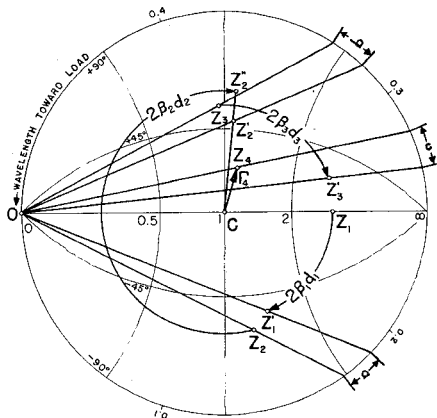


Fig. 2—Graphical construction for example.

point  $Z_1$  is rotated through the angle  $2\beta_1 d_1$  or  $(1.861)(0.05)\lambda = 0.093\lambda$  to obtain  $Z_1' = 1.40 / -54^\circ$ . The point  $Z_2 = (\eta_{1\perp}/\eta_{2\perp})Z_1' = 1.24 / -61.9^\circ$  is plotted. The point  $Z_2$  is rotated through the angle  $2\beta_2 d_2$  or  $(1.317)(0.21)\lambda = 0.278\lambda$  to obtain  $Z_2'$ . The distance  $\overline{CZ_2'} e^{-2\alpha_2 d_2} = \overline{CZ_2'} e^{-0.0303} = 0.739 \overline{CZ_2'}$  is meas-

ured from  $C$  along the line  $CZ_2'$  to locate the point  $Z_2'' = 1.07/49^\circ$ . The point  $Z_3 = (\eta_{2\perp}/\eta_{3\perp})Z_2'' = 0.96/56.9^\circ$  is plotted. The point  $Z_3$  is rotated through the angle  $2\beta_3 d_3$  or  $(1.485)(0.07)\lambda = 0.104\lambda$  to obtain  $Z_3' = 2.98/25^\circ$ . The point  $Z_4 = (\eta_{3\perp}/\eta_{3\perp})Z_3' = 1.13/25^\circ$  is plotted.

The magnitude of the voltage reflection coefficient is  $\overline{CZ_4}/(\text{radius of chart}) = 0.23$  Now

$$|E_4^+| = \frac{\overline{OC} \overline{OZ_1'} \overline{OZ_2'} \overline{OZ_3'}}{\overline{OZ_1} \overline{OZ_2} \overline{OZ_3} \overline{OZ_4}} e^{\alpha_1 d_1 + \alpha_2 d_2 + \alpha_3 d_3} = 1.10$$

and the ratio of power transmitted to power incident is 0.826. The angle of  $E_4^+$  is

$$a - b - c + \beta_1 d_1 + \beta_2 d_2 + \beta_3 d_3 = 360^\circ(0.014 - 0.016 - 0.016 + 0.093 + 0.278 + 0.104) = 164.5^\circ,$$

and the increase in phase retardation due to the sandwich is

$$\Phi = 164.5^\circ - (360^\circ/1.26)(0.33) \cos 45^\circ = 9.78^\circ.$$

A graphical construction for determining the transmission characteristics of a sandwich has the advantage that the effect of the individual layers is presented in visual form. Ways to vary the parameters to obtain a desired result may be suggested by a study of the chart.

H. F. MATHIS  
Goodyear Aircraft Corp.  
Akron, Ohio

### Measurement of Reflection Coefficients through a Lossless Network

Often it is not convenient to measure a reflection coefficient directly. In some such

cases, the following procedure may be used. The arrangement of components shown in Fig. 1 will be considered. It will be assumed that lines Nos. 1 and 2 are lossless. These lines may be transmission lines, waveguides, or one of each.

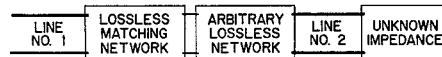


Fig. 1—Arrangement for measuring reflection coefficients.

First, a matched load is connected to line No. 2 and the matching network is adjusted until the reflection coefficient in line No. 1 is zero. Next, the matched load is replaced by a short circuit. The magnitude of the reflection coefficient in line No. 1 should be one. This should be checked experimentally. A voltage null in line No. 1 is located and designated the *short-circuit point*. Finally, the short circuit is replaced by the unknown impedance. The reflection coefficient  $\Gamma_1$  in line No. 1 is measured relative to the short-circuit point. The reflection coefficient  $\Gamma_2$  in line No. 2 related to the point where the short circuit was connected is the same as  $\Gamma_1$ .

The theoretical basis for this procedure is the well-known equation

$$\Gamma_1 = \frac{a\Gamma_2 + b}{c\Gamma_2 + d}$$

Since  $\Gamma_1 = 0$  when  $\Gamma_2 = 0$ ,  $b = 0$ . Since the various components are lossless,  $\Gamma_1 = 1$  when  $\Gamma_2 = 1$ . Consequently,  $|c\Gamma_2 + d|$  is equal to a constant for all values of  $\Gamma_2$  such that  $\Gamma_2 = 1$ . This requires that  $c = 0$ . Now  $\Gamma_1 = (a/d)\Gamma_2$ , where  $a/d = 1$ . When  $\Gamma_1$  is referred to the short-circuit point,  $a/d = 1$  and  $\Gamma_1 = \Gamma_2$ .

H. F. MATHIS  
Goodyear Aircraft Corp.  
Akron, Ohio

## Contributors

A. Clavin (A'51) was born in Los Angeles, Calif., June 17, 1924. He received his B.S. degree in electrical engineering from U.C.L.A. in 1948 and became a member of the technical staff of Hughes Aircraft Co. During his six years there, he concerned himself with the design of microwave components, antennas and radomes.



A. CLAVIN

Mr. Clavin received his M.S. degree in 1954 from U.C.L.A. and joined

Litton Industries, where he worked on the development of ferrite microwave components. Later that year he became a senior antenna and microwave engineer at Canoga Corp., where he has continued his work in the development of ferrite components.



For a photograph and biography of S. B. Cohn, see the March, 1955 issue of the TRANSACTIONS OF THE IRE-PGMMT.



B. A. Dahلمان graduated from the Royal Institute of Technology in Stockholm, Sweden, in 1951. He served in the



B. A. DAHLMAN

and transistors. Mr. Dahلمان returned to Sweden in 1954 and is now with Magnetic AB in Stockholm.

Swedish Navy for one year, and while in service was engaged in radar work at the Research Institute of National Defense.

He continued his radar studies until 1952 when he joined the RCA Laboratories at Princeton, N. J. for research on microwave circuits